

Smart Base Station Antenna Performance for Cellular Radio System

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Abstract

Adaptive array antenna technology is useful for detecting the Direction of Arrival (DOA) of signal and delay for mobile communications, where the antenna beam will automatically directed to the signal source. One method to estimate DOA and delay effectively is by using MUSIC (Multiple Signal Classification) algorithm. When the signal arrive at the antenna, the MUSIC algorithm will arrange the signal into its matrix covariance, and then perform an eigen decomposition process to produce the signal and noise subspace, and then obtain the power spectrum and delay spectrum.

This paper combined the Taguchi method and MUSIC algorithm, used them as the prediction tool in designing parameters for the communication system and then constructed a set of the optimal parameter analysis flow and steps. Several adaptive beamforming criteria were discussed and a general form for the optimum array weight vector was derived that would require large amounts of computational load. Hence, it is necessary to find technique that can find optimum solution in real time. This paper will discuss the application of MUSIC algorithm for linear and circular array antenna in order to estimate the DOA and delay of various angles of elevation and azimuth.

Keywords: Taguchi, phased antenna array, Steering beams, MUSIC, TDOA, DOA, Interference nulling.

1. Introduction

ABASE transceiver station (BTS) is a piece of equipment that facilitates wireless communication between user equipment (UE) and a network. UEs are devices like mobile phones, WLL phones, computers with wireless internet connectivity, WiFi and WiMAX devices and others. The network can be that of any of the wireless communication technologies like GSM, CDMA, Wireless local loop, WAN, WiFi, WiMAX, etc.

With the advent of mobile high-speed data applications, it is expected that the downlink of 3G CDMA systems will be the limiting link as far as capacity is concerned. Hence, it is important to investigate methods that can increase the downlink capacity to cope with increasing demand.

In cellular systems such as GSM or IS-95, antenna arrays can be used at base stations (BSs) to increase user capacity and provide other advantages such as improving voice quality, extending battery life in handsets and increasing data transmission rates. Array antennas have been employed in military systems for many years as a counter measure for deliberate, high power jammers [1].

Smart antenna systems are employed to overcome multipath fading, extend range, and increase capacity by using diversity or beamforming techniques in wireless communication systems [2]. Understanding of the smart base antenna performance mechanisms for various

environments is important design cost effective systems and networks. This dissertation focuses on the experimental characterization and modelling of the smart base station antenna performance for various propagation environment scenarios. In [3] the author's describes a mobile communication base station antenna using a genetic algorithm based Fabry-Pérot resonance optimization. Their focal contribution is a beamformer-power update algorithm based on uplink-downlink duality that converges to a feasible solution to the problem. In the single-cell multi-user downlink case, the optimality of their algorithm was later proved by Visotsky and Madhow[4] and Schubert and Boche[5], [6]. Recently, Wiesel, Eldar and Shamai[7] showed that the single cell downlink beamforming problem can be formulated as a second-order cone-programming problem. In [8] the author's describes the smart antenna along with spatial diversity using fuzzy interference system and neural network (NN). In order to provide training for NN and fuzzy logic, a huge personalised training dataset is generated using Genetic Algorithm.

In this paper, a global optimization technique based on Taguchi method and MUSIC (Multiple Signal Classification) algorithm are applied so as to determine the excitation coefficients and the resultant pattern for a broadside discrete element array whose array factor will directly approximate the symmetrical sectoral pattern in order to estimate the DOA and delay of various angles of elevation and azimuth. The implementation system is described in detail, and linear antenna array examples are discussed to demonstrate its validity. Optimized results show

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that the desired array factors, a null controlled pattern and a sector beam pattern, are effectively obtained. It is found that neural network is an excellent candidate for optimizing diverse applications, as it is easy to realize and converges to the desired patterns rapidly. The paper is organized as follows. The synthesis problem formulation using Taguchi method is presented in section II. Multilayer Networks and Back-Propagation Algorithm is developed in section III. Section IV shows the novel design of phased antenna array with the simulation and measurement result, finally, section V makes conclusions.

2. Statement of Problem

Adaptive array systems can locate and track signals (users and interferences) and dynamically adjust the antenna pattern to enhance reception while minimizing interference using signal-processing algorithms. A functional block diagram of such a system is shown in Fig 1 and Fig 2. This Figures show that after the system down converts the revised signals to baseband and digitizes them, it locates the SOI using the direction-of-arrival (DOA) algorithm, and it continuously tracks the SOI and SNOIs by dynamically changing the weights (amplitudes and phases of the signals). Basically, the DOA computes the direction of arrival of all signals by computing the delays between the antenna elements, and afterward the adaptive algorithm, using a cost function, computes the appropriate weights that result in an optimum radiation pattern.

In this section, a description of the system model used in the simulation and the analytical study is presented.

2.1. Digital Beam-Steering

We present in this section an electronic platform dedicated to the implementation of adaptive array antenna. Functional Block Diagram of a smart antenna system as shown in Figure 1.

This scheme employs directional antennas as array elements. These elements are placed in such a way that the combined array pattern covers the region of interest. At an instant the antenna with highest receive signal strength is selected by switch. One of the advantages of this system is the computational simplicity; the switching system scans the antennas and selects the antenna with highest receive signal strength, which also results in higher tracking speed. Low cost advantage of this system because a down converter and an analog-to-digital converter (ADC) with one channel is sufficient at the receiver side. As the beam pattern of the same antenna. In adaptive beamforming, weights used for combining the antennas can be adaptively calculated and adjusted to achieve greater performance improvements than what is possible when using switched antenna systems. An adaptive beamforming block diagram is shown in Figure x. In this Figure, the desired signal corresponds to a local generated replica of the user's signal obtained using a predetermined training sequence based on MUSIC Algorithm with Adaptive Taguchi synthesis method.

2.2. Cellular Radio System Evolution

The basic function of macro cell base station antenna is to provide uniform coverage in the azimuth plane, but to provide directivity in the vertical plane, making the best possible use of the input power by directing in at the ground rather than the sky [9]. If fully omnidirectional coverage is required, vertical directivity is usually provided by creating a

vertical array of antennas, phased to give an appropriate pattern. More commonly in cellular mobile systems, however, some limited azimuth directivity is required in order to divide the coverage area into sectors. A typical example is shown in Figure . The choice of the azimuth beam width is trade-off between allowing sufficient overlap between sectors, permitting smooth handovers, and controlling the interference reduction between co-channel sites, which is the main point of sectorization.

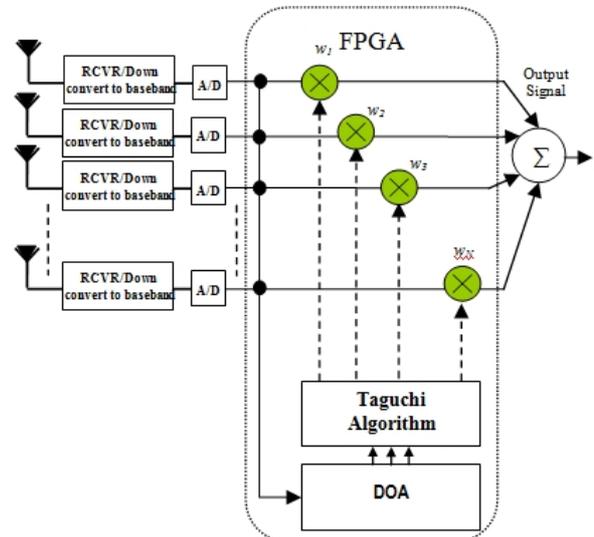


Fig.1. Functional block diagram of an adaptive array system

Objects surrounding the BS and MS severely affect the propagation characteristics of uplink and downlink channels of cellular systems. This propagation path loss, including reflection and shadowing, tends to degrade system capacity. The height of the MS antenna is normally much lower than that of the surrounding building and natural features. Furthermore, the carrier frequency wavelength is also much less than the size of the surrounding structures. Due this, the MS will experience significant charges of its received signal strength as it moves [1].

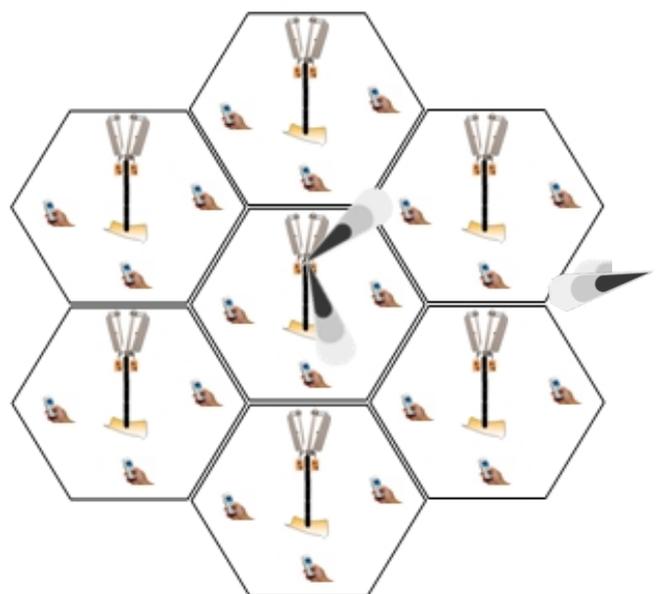


Fig.2. A wireless network with seven base-stations and three users per cell.

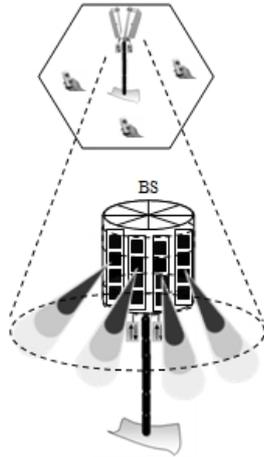


Fig. 3.A wireless network with seven base-stations and three users per cell.

3. Signal Model and Estimation Algorithm

3.1 Multiple Signal Classification

Consider that the array antenna used for DOA estimation is a K -element linear array shown in Fig.1, and also that it receives L ($L < K$) narrow-band waves whose respective DOAs are $\theta_1, \theta_2, \dots, \theta_L$ and complex amplitudes are $s_1(t), s_2(t), \dots, s_L(t)$.

When the array response vector (mode vector) of the l th incoming wave is given by $a(\theta_l)$ ($l = 1; 2; \dots; L$), the array input vector $x(t)$ can be expressed as

$$x(t) = \sum_{k=1}^d s_k a(t_k, u_k) + n \quad (1)$$

$$x(t) = As + n \quad (2)$$

$$x(t) = \sum_{l=1}^L a(\theta_l) s_l(t) + n(t) = As(t) + n(t) \quad (3)$$

When $x(t)$ and $n(t)$ are column vectors of size $[MF, 1]$ (M : number of antennas and F : number of frequency points), and a matrix A with dimensions $[MF, d]$ whose columns are the vectors $a(t_k, u_k), 1 \leq k \leq d$ defined by:

$$a(t_k, u_k) = \begin{bmatrix} e^{-2.j.\pi.(f_1.t_k - g_1.u_k)} \\ e^{-2.j.\pi.(f_2.t_k - g_2.u_k)} \\ \dots \\ e^{-2.j.\pi.(f_r.t_k - g_r.u_k)} \\ e^{-2.j.\pi.(f_1.t_k - g_1.u_k)} \\ e^{-2.j.\pi.(f_2.t_k - g_2.u_k)} \\ \dots \\ e^{-2.j.\pi.(f_r.t_k - g_r.u_k)} \\ \dots \\ e^{-2.j.\pi.(f_s.t_k - g_s.u_k)} \\ \dots \\ e^{-2.j.\pi.(f_f.t_k - g_f.u_k)} \end{bmatrix} \quad \forall 1 \leq k \leq d \quad (4)$$

$$A = [a(t_1, u_1), a(t_2, u_2), \dots, a(t_F, u_F)] \quad (5)$$

$$S = [s_1(t), s_2(t), \dots, s_L(t)]^T \quad (6)$$

With

$$g_m \approx \frac{f_0 \cdot x_m}{c}, \quad \forall 1 \leq m \leq M \quad (7)$$

$$u_k = \sin \phi_k, \quad \forall 1 \leq k \leq d \quad (8)$$

where A and $s(t)$ are called the array response matrix (mode matrix) and the signal vector, respectively, and $n(t)$ is the internal additive noise vector [10]-[11].

The elements $X(t)$ and A are generally complex. A is a matrix dimension $[M.F, d]$ whose columns $a(t_k, u_k)$ can be put in the form of Kronecker products:

$$a(t_k, u_k) = a_u(u_k) \otimes a_t(t_k) \quad (9)$$

where

$$a_u(u_k) = \begin{bmatrix} e^{2.j.\pi.g_1.u_k} \\ \dots \\ e^{2.j.\pi.g_m.u_k} \\ \dots \\ e^{2.j.\pi.g_M.u_k} \end{bmatrix} \quad \text{and}$$

$$a_t(t_k) = \begin{bmatrix} e^{-2.j.\pi.f_1.t_k} \\ \dots \\ e^{-2.j.\pi.f_r.t_k} \\ \dots \\ e^{-2.j.\pi.f_s.t_k} \end{bmatrix}, \quad \forall 1 \leq k \leq d$$

The k th column is a known function of the direction of arrival and relative time delay of the k th path.

The same element of the vector $a_u(u_k)$, $1 \leq m \leq M$, depends on the relative position of the same sensor, the f th element of the vector $a_t(t_k)$, $1 \leq f \leq F$, depends on the f th frequency.

3.2. MUSIC Algorithm

The most common techniques for DOA estimation can be distinguished between spectral based and parametric algorithms. Spectral based algorithms use a function, called pseudo spectrum, in which the maxima give an indication of the DOAs.

A large number of spectral based solutions have been proposed in literature, such as the Bartlett method, the Capon estimate, the linear prediction method, the maximum entropy method and many others [37].

A simple and widely adopted technique is the Multiple Signal Classification (MUSIC) algorithm, which exploits the eigen structure properties of the array correlation matrix [38].

MUSIC (standing for multiple signal classification) is generally used in signal processing problems as a method for estimating the individual frequencies of multiple-harmonic signals. This is also the most frequently studied in the

literature, evidently with MUSIC see [12]-[13]-[14] and [15].

The MUSIC algorithm is the high-resolution method based on the eigenvectors of the covariance matrix of the array input vector. The covariance matrix is given by

$$R_{xx} = E[x(t)x^H(t)] = ASA^H + \sigma^2 I \quad (10)$$

where $S = E[s(t)s(t)^H]$ and σ^2 is the power of internal noise. Then, the MUSIC spectrum is expressed as

$$P_{MUSIC}(t, u) = \frac{a(t, u)^H \cdot a(t, u)}{\sum_{k=d+1}^{M.F} |a(t, u)^H \cdot w_k|^2} \quad (11)$$

$$= \frac{|a(t, u)|^2}{\sum_{k=d+1}^{M.F} |a(t, u)^H \cdot w_k|^2}$$

$$P_{MU}(\theta) = \frac{a(\theta)^H a(\theta)}{a(\theta)^H E_N E_N^H a(\theta)} \quad (12)$$

$$E_N = [e_{L+1}, \dots, e_K]$$

where E_N is composed of the eigenvectors: $\{e_{L+1}, \dots, e_K\}$ spanning the noise subspace of the covariance matrix

R_{xx} .

3.3. Results and Discussion

In this section, computer simulation results are provided to assess the performance with MUSIC Algorithm with different angles (AOA) and Time of arrivals (TDOA).

The MUSIC algorithm is implemented in MATLAB and tested by giving different angles as input to the system.

In this example, we show the TOA and the DOA simulation results in azimuth and in elevation plane by using a Matlab code. The simulation performed is based on the use of MUSIC algorithm. Figs. 4 and 5 show the MUSIC spectrum for uniform linear array with 10 elements and SNR=31.62 dB, K=100 for direction of arrivals @60°, 40°, 20°, -10°, -30° and -50° degrees. Spacing between elements is assumed to be 0.5λ with time delay TDOAs=10, 13, 17, 20, 27 and 35 ns and Time delay TDOAs =10, 35 and 20 ns in Fig.7.

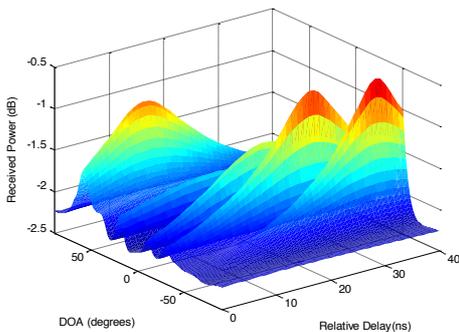


Fig. 4. Pseudo spectrum with SNR = 31.6228 and angles (@60°, @ 40°, @ 20°, @ -10°, @ -30° and@ -50°). Time delays (10ns, 13ns, 17ns, 20ns , 27ns and 35ns) with 10 antennas

Similarly, Fig.6 shows the array factor obtained using the N = 10 antennas; this Figure shows the beam patterns synthesis by Taguchi Method when the AOA of the incoming signal is changed between 60° and -50°. Again , AOA is correctly found by the synthesis weights. So from these results, we can predict synthesis weights. Finally, this method present a good beam scanning performance with the gain variation is below 3dB within the beam scanning volume between @-90° and @+90°.

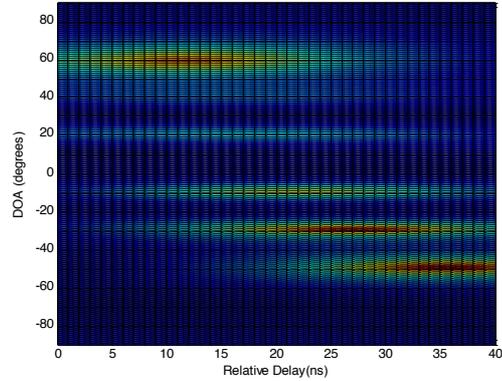


Fig. 5. Tomography image with SNR = 31.6228 and angles (@60°, @ 40°, @ 20°, @ -10°, @ -30° and@ -50°). Time delays (10ns, 13ns, 17ns, 20ns, 27ns and 35ns) with 10 antennas

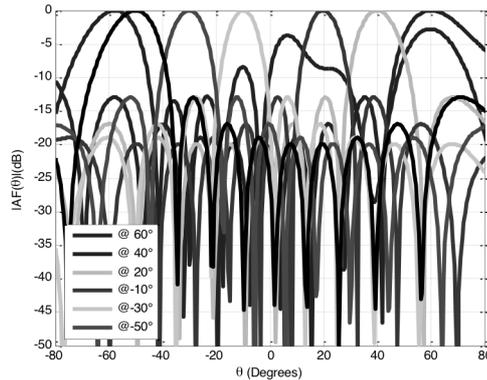


Fig.6. Radiation pattern of 10 elements λ/2 spaced array optimized using Taguchi.

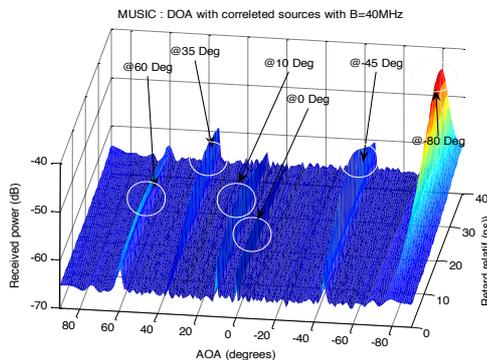


Fig. 7. Pseudo spectrum with SNR = 31.6228 and angles (@60°, @ 35°, @10°, @0°, @-45° and@ -80°)

4. Electromagnetic Optimization Using Hybrid Beamforming Taguchi-Music Algorithm

The radiation characteristics of antennas have mostly to do with the far field region. In this region, the field expression

is a multiplication of two parts. One part contains the distance r dependence of the observation point and the other contains its spherical coordinate angles θ and φ dependence.

The angular distribution of the field is independent of the distance r . For a typical antenna element, the far electric field is

$$E_n(r) \cong -j\omega\mu \frac{e^{-j\beta r}}{4\pi r} f_n(\theta, \varphi) \quad (13)$$

The angular-dependent vector $f_n(\theta, \varphi)$ gives the directional characteristics of the n th element electric field [17]-[18]:

$$f_n(\theta, \varphi) = I_n f(\theta, \varphi) \quad (14)$$

$f(\theta, \varphi)$ is called the 'pattern function' of the element and I_n is the complex excitation of the n th element of the array.

$$E(r) \cong -j\omega\mu \frac{e^{-j\beta r}}{4\pi r} f(\theta, \varphi) \sum_{n=1}^N I_n e^{j\beta r_n \cos \xi_n} \quad (15)$$

Where

r = distance of the observation point from the origin

$\beta = \frac{2\pi}{\lambda}$ the free space wave number

ω = the angular frequency and

μ = the magnetic permeability of the space

$(r_n, \theta_n, \varphi_n)$ are the spherical coordinates of a convenient reference point of the n th element and

$$\cos \xi_n = \sin \theta \sin \theta_n \cos(\varphi - \varphi_n) + \cos \theta \cos \theta_n \quad (16)$$

4.1 Taguchi Optimization Method

In Fig.8, every step in the flowchart will be generally explained, and then they will be applied on some examples to show the efficiency of this technique.

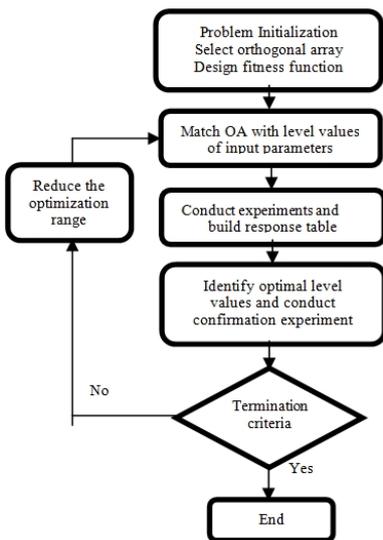


Fig. 8. Flow chart of Taguchi method [22]-[23]

In this example, Taguchi's optimization method will be applied on a 10-element linear array. Table I (Phase

synthesis values) and Table II (amplitude values) hold the optimum values of the phase and amplitude obtained using Taguchi's method (after 100 iterations). A Laptop with Intel Core (TM) 2 Duo CPU@2.00 GHz and 2.96 Go RAM were used for simulating the Taguchi's code, and the simulation time was only 12 seconds.

a.1. Initializing the Problem

a.2. Designing Input Parameters Using an OA

$$LD_1 = \frac{(\max - \min)}{s + 1} \quad (17)$$

where "max" and "min" are the upper and lower bounds of the optimization range, respectively.

a.3. Conducting Experiments

$$\eta = -20 \log(\text{Fitness}) \text{ (dB)} \quad (18)$$

After conducting all the experiments and finding the fitness values and the corresponding S/N ratio, a response table is built by averaging the S/N for each parameter n and level m using [19]-[22].

$$\bar{\eta}(m, n) = \frac{1}{N_{i, OA(i, n) = m}} \sum \eta_i \quad (19)$$

a.4. Identifying Optimal Level Values and Conducting Confirmation Experiment

a.5. Reducing the Optimization Range

If the termination criteria are not satisfied, the optimal level for the current iteration will be the center of the next iteration.

$$\varphi_n \Big|_{i+1}^2 = \varphi_n \Big|_i^{opt} \quad (20)$$

Also, the optimization range for the next iteration is minimized by multiplying the current level difference by the reducing rate (rr) eq.5. rr can be set between 0.5 and 1 according to the problem [3]. So, for the $(i+1)^{\text{th}}$ iteration [22]-[23].

$$LD_{i+1} = RR(i) \times LD_1 = rr^i \times LD_1 \quad (21)$$

Where $RR(i) = rr^i$ is called the reduced function.

a.6. Checking the Termination Criteria

$$\frac{LD_{i+1}}{LD_1} \leq \text{converged value} \quad (22)$$

Usually, the converged value can be set between 0.001 to 0.01 depending on the problem. If the design targets are achieved or Eq. 21 is satisfied, the optimization process will finish. Finally, the above steps are repeated until a specific termination criterion is achieved or a specific number of iterations are reached.

4.2 Linear antenna array

Usually, in the design of an antenna array, some constraints, such as the SLL, the FNBW, the HPBW and the directivity,

are specified, while others, such as the phase/amplitude of the elements, the number of radiators and the geometry of the array, must be properly derived to satisfy the design requirements.

Which has $N=10$ equally spaced elements along the axis x . The element spacing is half-wavelength and the excitations of array elements are symmetric with respect to the axis y . The excitation amplitude of the five elements will be optimized in the range of (0, 1) to shape the antenna pattern.

For a 10 element symmetrical array, the array factor can be written as [20]-[21]-[22]:

$$E(r) \cong -j\omega\mu \frac{e^{-j\beta r}}{4\pi r} f(\theta, \varphi) AF(\theta, \varphi) \quad (23)$$

$$E(r) \cong -j\omega\mu \frac{e^{-j\beta r}}{4\pi r} f(\theta, \varphi) \times \left(2 \sum_{n=1}^N A(n) e^{j\varphi(n)} \cos[kd(n)\cos\theta] \right) \quad (24)$$

where k is the wave number; $A(n)$, $d(n)=\lambda/2$, and $\varphi(n)=0$ are the excitation amplitude, location, and phase of the n^{th} element, respectively.

The following fitness function can be used in the optimization.

$$fitness = \min(\max\{20 \log|AF(\theta)|\}) \quad (25)$$

The array factor can be written as

$$AF(\theta) = 2 \sum_{n=1}^5 A(n) e^{j\varphi(n)} \cos[kd(n)\cos\theta] \quad (26)$$

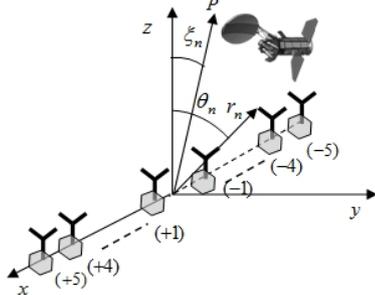


Fig.9. Geometry of an antenna array with 10 identical elements

4.3 Circular antenna array

Another commonly employed configuration is the Uniform Circular Array (UCA), in which the elements are regularly arranged on a circular ring (Fig. 1.6). The UCA is of very practical interest and is often adopted in radar and sonar systems as well as in cellular base stations.

Besides, a direct comparison between a UCA (Uniform Circular Array) and a ULA (Uniform Linear Array) shows that, adopting the same number of elements and the same spacing between adjacent radiators, the circular array produces narrower main beams with respect to the corresponding linear array. The performance of the circular configurations can be improved by using multiple rings in

order to obtain a Concentric Ring Array (CRA). This planar geometry enables the scanning in both azimuth and elevation planes [35]-[36].

Let us first make some elementary observations of the differences between linear and circular arrays. For the linear array in Fig.10, the radiating elements are identical, with equal spacing d , and they all point in the same direction. The far-field radiation function is [5]:

$$E_n(r, \theta, \varphi) = \frac{e^{-jkr}}{r} \sum_{n=1}^N V_n e^{jka \sin\theta \cos(\varphi - \varphi_n)} \quad (27)$$

Where,

V_n is the excitation amplitude of element n

k is the propagation constant, $k = 2\pi / \lambda$

$\varphi_n = 2\pi(\frac{N}{n}) = \text{Angular position of } n\text{th element}$

In general, the excitation coefficient of the n th element can be written as

$$V_n = I_n e^{-ja_n} \quad (28)$$

Where

$I_n = \text{Amplitude excitation on the } n\text{th element,}$

$a_n = \text{Phase excitation (relative to the array center) of the } n\text{th element.}$

$$E_n(r, \theta, \varphi) = \frac{e^{-jkr}}{r} [AF(\theta, \varphi)] \quad (29)$$

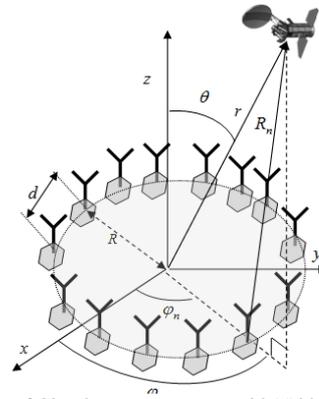


Fig.10. Geometry of Circular antenna array with N identical elements

Thus, the radiation function for the focused, circular case becomes

$$AF(\theta, \varphi) = \sum_{n=1}^N I_n e^{j[kR \sin\theta \cos(\varphi - \varphi_n) + a_n]} \quad (30)$$

With the circular array, we can similarly impose phase values to each element so that they add up coherently in the direction θ_0 . We get the proper phase excitation for each element n by choosing [26]-[27]-[28].

$$\alpha_n = -kR \sin \theta_0 \cos(\theta_0, \varphi_n) \tag{31}$$

Thus the array factor can be written as

$$AF(\theta, \varphi) = \sum_{n=1}^N I_n e^{jkR[\sin \theta \cos(\varphi - \varphi_n) - \sin \theta_0 \cos(\varphi_n - \varphi_s)]} \tag{32}$$

$$= \sum_{n=1}^N I_n e^{jkR[\cos \psi - \cos \psi_n]}$$

For conformal arrays, the element pattern plays an important role in the array pattern, because each element is facing a different direction. Which has 10 equally spaced elements. The element spacing is half-wavelength and the excitations of array elements are symmetric with respect to the axis y. The excitation amplitude of the five elements will be optimized [19]-[22] in the range of (0, 1) to shape the antenna pattern. One of the major advantages of array antennas is that the array excitation can be closely controlled to produce extremely-low-side lobe patterns or very accurate approximations of chosen radiation patterns. Many intricate procedures have been developed for synthesizing useful array factors. These methods fit into three main classes of synthesis: synthesis of various sector patterns that are usually many beam widths wide, synthesis of low-side lobe, narrow-beam patterns, and procedures that optimize some array parameter, such as gain and signal to-noise ratio, subject to some constraint on the side lobe level or the existence of outside noise sources. To illustrate the effectiveness of the proposed approach, two examples are presented here. In the examples, the Taguchi optimization technique is carried out in ten runs of 100 iterations each. For these two examples, the CPU time for 100 iterations is about 6.5s using MATLAB software on an Intel(R) Core (TM) i3-2370M CPU @ 2.4 GHz PC.

In this example (#1), Taguchi's optimization method will be applied on a 10-element linear array (example #1). Table III holds the optimum values of the amplitudes obtained using Taguchi's method (after 100 iterations). In this section, Taguchi algorithm is implemented for the equally spaced symmetric circular array. The problem is to optimize the amplitudes of the elements to achieve minimum SLL or/and with null placement.

For this antenna arrays, different numbers of elements are taken. The amplitudes of the elements allowed to vary between [0; 1].

The notation OA is used to represent an orthogonal array [10]. To help readers understand the OA definition, Table I shows an orthogonal array OA(27, 10, 3, 2), which has 27 rows and 10 columns. Each entry of the array is selected from a set $s=\{1,2,3\}$. Thus, this is a three-level orthogonal array. choose any two columns, and one may see nine possible combinations as a row [22]-[23]: (1, 1), (1, 2), (1, 3), (2, 1), (2, 2), (2, 3), (3,1), (3, 2), (3, 3). It can be easily proved that each combination appears exactly the same number of times as a row, i.e., three times[24]-[25].

In this section, we consider a circular array of 10 isotropic elements spaced 0.5λ apart in order to generate two beams towards the steering angles @30°, @150° with amplitude-phase synthesis by Taguchi method. Because of symmetry, here only five phases and five amplitudes are to be optimized. Acceptable Side Lobe Level (SLL) should be equal to or less than the desired value @- 40dB.

We often want that the side lobe level is as low as possible. We shall apply the optimized weights before, the amplitudes to minimize them and the phases to direct the main lobe.

When this optimization process has been executed for 100 iterations, an optimal control pattern is obtained and presented in Fig. 11.Taguchi method was used to adjust the position and the excitation of each element in the circular array to obtain better side lobe suppression.

Table 1. The OA(27, 10, 3, 2), Fitness Values, And S/N Ratios In The First Iteration Of The Null Controlled Pattern Optimization

Experiences	Element #					fitness	RS/N
	V ₁	V ₂	V ₃	V ₄	V ₅		
1	0.25	0.25	0.25	0.25	0.25	7.9	-17.95
2	0.5	0.25	0.5	0.5	0.5	8.84	-18.93
3	0.75	0.25	0.75	0.75	0.75	9.15	-19.22
4	0.25	0.5	0.25	0.5	0.5	11	-20.83
5	0.5	0.5	0.5	0.75	0.75	10.76	-20.67
6	0.75	0.5	0.75	0.25	0.25	3.87	-11.75
7	0.25	0.75	0.25	0.75	0.75	12.89	-22.20
8	0.5	0.75	0.5	0.25	0.25	4.2	-12.47
9	0.75	0.75	0.75	0.5	0.5	5.83	-15.31
10	0.25	0.25	0.5	0.25	0.5	6.45	-16.19
11	0.5	0.25	0.75	0.5	0.75	7.49	-17.49
12	0.75	0.25	0.25	0.75	0.25	12.7	-22.1
13	0.25	0.5	0.5	0.5	0.75	9.06	-19.14
14	0.5	0.5	0.75	0.75	0.25	9.7	-19.72
15	0.75	0.5	0.25	0.25	0.5	4.92	-13.85
16	0.25	0.75	0.5	0.75	0.25	11.34	-21.1
17	0.5	0.75	0.75	0.25	0.5	4.42	-12.91
18	0.75	0.75	0.25	0.5	0.75	7.03	-16.94
19	0.25	0.25	0.75	0.25	0.75	5.37	-14.6
20	0.5	0.25	0.25	0.5	0.25	10.7	-20.58
21	0.75	0.25	0.5	0.75	0.5	10.64	-20.54
22	0.25	0.5	0.75	0.5	0.25	7.97	-18.03
23	0.5	0.5	0.25	0.75	0.5	12.83	-22.16
24	0.75	0.5	0.5	0.25	0.75	4.95	-13.89
25	0.25	0.75	0.75	0.75	0.5	9.91	-19.93
26	0.5	0.75	0.25	0.25	0.75	5.52	-14.84
27	0.75	0.75	0.5	0.5	0.25	5.85	-15.35

Table. 2. Response Table in the First Iteration of Null Controlled Pattern Optimization

	Element (dB)				
	V ₁	V ₂	V ₃	V ₄	V ₅
Level 1	-18.89	-18.62	-19.05	-14.27	-17.67
Level 2	-17.75	-17.78	-17.58	-18.06	-17.85
Level 3	-16.55	-16.78	-16.55	-20.84	-17.66

We have presented a pattern synthesis method of uniform circular antenna arrays for simultaneous reduction of the side lobe level, required smaller circumference and nearly symmetrical pattern. The result shows the circular antenna array radiation pattern at @30° and @150°, the Side Lobe Level (SLL) is -41.0495 dB. The optimized excitation magnitudes of elements are listed in Table III. To appreciate the efficiency of Taguchi's method, the convergence curve of fitness value is plotted in Fig. 12. It is observed that the fitness value converges to the optimum result quickly. Results clearly show a very good agreement between the desired and synthesized specifications.

The Taguchi method in example (#1) used to obtain the voltages (Amplitude and phase) corresponding to the specified near field distribution. The resulting voltages, listed in Table II and present the optimized element excitations of the circular antenna array with a sector beam pattern shown in Fig. 11.

The optimization ranges of the excitation magnitude and phase of each element are from zero to one and from to, respectively. Eq.(21) is used for evaluating the fitness value during the optimization process. The converged value is set to 0.001 and the RR is set to 0.9.[22].

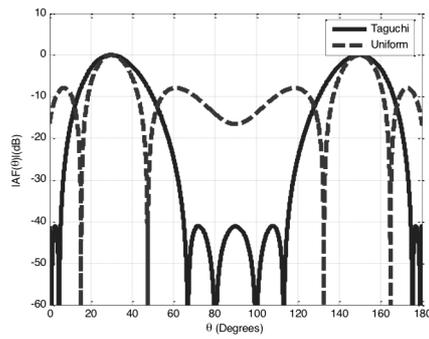


Fig. 11. Radiation pattern for N = 10 using the Taguchi results as compared to the uniform results

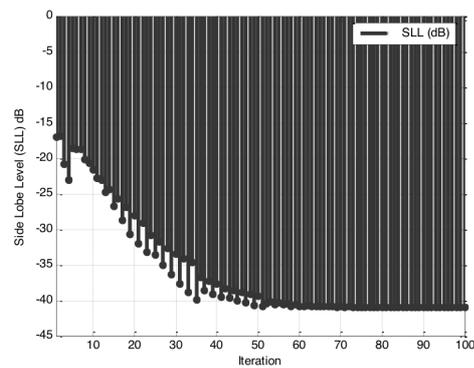


Fig. 13. Convergence curve of Side Lobe level reduction of the 10-element equally spaced linear array for the controlled pattern design with Taguchi Method.

For the next examples (#2 and #3), we take an array with 24 elements, in amplitude-phase synthesis, the design of this array is based on finding the amplitude and phase distribution of each element, in the plane $\phi=90^\circ$, the SLL is set to -8dB (example #2), and the SLL is set to -27 dB (example #3). So to illustrate the performance of the method described in the earlier section for steering single and multiple beams in desired direction by controlling the amplitude and phase excitation of each array element, 2 examples of Taguchi excited circular array with N = 24, one-half wavelength spaced isotropic elements were performed with the main beam pointing at 18 directions. Fig.14 and Fig.15 show a synthesis radiation pattern with Taguchi method, which illustrates the above discussion on how the beam is steered to a desired angle θ_0 starting from T_1 until T_{18} ($\theta_0 = 0^\circ, 10^\circ, 20^\circ, 30^\circ, 40^\circ, 50^\circ, 60^\circ, 70^\circ, 80^\circ, 90^\circ, 100^\circ, 110^\circ, 120^\circ, 130^\circ, 140^\circ, 150^\circ, 160^\circ, 170^\circ, 180^\circ$).

Table. 3. Synthesized Voltages, Example #1

Element #	Element (dB)	
	Amplitude	Phase (deg.)
1	0.2015	93.863
2	0.1452	75.008
3	0.367	165.03
4	1	-30.496
5	0.6182	145.62
6	0.6182	-145.62
7	1	30.496
8	0.367	-165.03
9	0.1452	-75.008
10	0.2015	-93.863

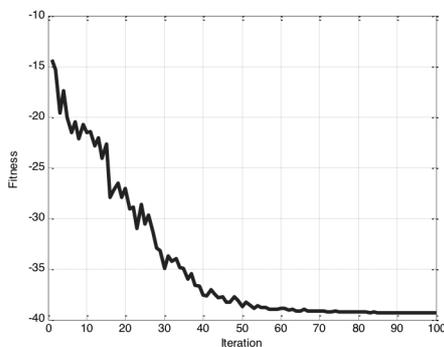


Fig. 12. Convergence curve of the fitness value of the 10-element equally spaced linear array for the controlled pattern design.

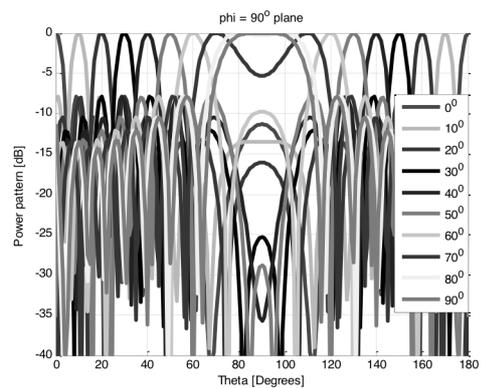


Fig. 14. Radiation pattern for N = 24 using the Taguchi results example#2

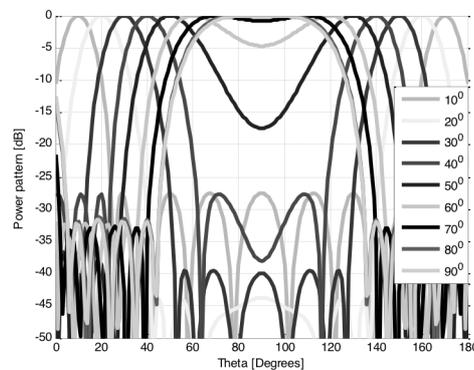


Fig.15. Radiation pattern for N = 24 using the Taguchi results example#3

The results of steering beam in the direction of the desired signal are presented in Figs 13 and 14 with the converged value is set to 0.001 and the RR is set to 0.9; this result is obtained after 100 iterations. This property of the proposed design enables to choose the size (area) of the region to be covered by the main beam while keeping radiation in the other directions below a desired level.

Fig.17 gives the computed element phases by Taguchi method (example#3).

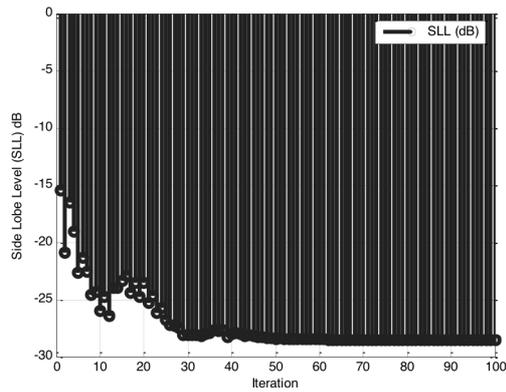


Fig. 16. Convergence curve of Side Lobe level reduction of the 24-element equally spaced linear array for the controlled pattern design with Taguchi Method (example#3).

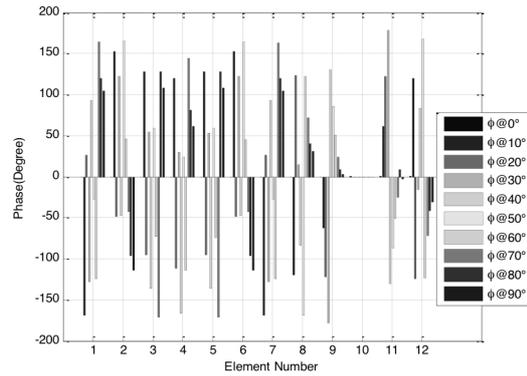


Fig. 17. Optimized element excitations (Phases) of the circular antenna array by Taguchi method (example#3)

In this session , the Taguchi method was used to adjust the position and the excitation of each element in the circular array to obtain better side lobe suppression. We have presented a pattern synthesis method of circular antenna arrays for simultaneous reduction of the side lobe level, required smaller circumference and nearly symmetrical pattern. Array patterns obtained from Taguchi results are generally better than those presented in [29] which were obtained using GA. At the present time, we are investigating the application of the PSO method to optimize the side lobe level of concentric circular arrays [33]-[34].

Table. 4. Synthesized Voltages, Example #3

Element #	Element (dB)
	Amplitude
1&24	0.3015
2&23	0.0157
3&22	0.0166
4&21	0.2641
5&20	0.0091
6&19	0.0105
7&18	0.4056
8&17	0.4450
9&16	0.8339
10&15	1.0000
11&14	0.9772
12&24	0.5883

5. CONCLUSION

In this paper, we propose a hybrid optimization approach that combines the MUSIC (Multiple Signal Classification) algorithm with Taguchi's method.

In adaptive array smart antenna, to locate the desired signal, various DOA estimation algorithms are used. Most of the DOA estimation algorithms are applied in the antenna array assumed to be isotropic point sources which are impractical. The simulation results illustrate that the MUSIC and Taguchi method for DOA estimation can be applied on real time with array elements. Many numerical examples were introduced to measure the performance of the both algorithms and their ability to resolve incoming signals accurately and efficiently. The performance of the MUSIC algorithm depends on the number of the data snapshots. The MUSIC algorithm has highly accurate and stable and provides high angular resolution. The advantage of Taguchi's optimization technique is the ability of solving problems with a high degree of complexity using small number of experiments in the optimization process. Taguchi's method is easy to implement and converges to the desired goal quickly. To demonstrate this technique, a linear antenna array is optimized to realize a null control pattern and a sector beam pattern.

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